

Voltage Clamped Dc-Dc Converter with Reduced Reverse Recovery Current And Stability Analysis

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Abstract: this paper in vest gates a high-efficiency clamped-voltage dc-dc converter with reduced reverse-recovery current And switch-voltage stress. In the circuit topology, it is designed by way of the combination of in duct or and transformer to increase the corresponding voltage gain. Moreover, one additional inductor provides the reverse-current path of the transformer to enhance the utility rate of magnetic core. In addition, the voltage-clamped technology issued to reduce the switch-voltage stress so that it can select the Scotty diode in the output terminal for all aviating the reverse recovery current and decreasing the witching and conduction losses. Fur the more; the closed-loop control methodology is utilization the proposed scheme to overcome the voltage-drift problem of power source under the variation of loads. Thus, the proposed converter topology has a favor able voltage-clamped effect and superior conversion efficiency. Some experimental results via an example of a proton exchange membrane fuel cell (PEMFC) power source with a 250-W nominal rating are given to demonstrate the effectiveness of the proposed power-conversion strategy.

Index Terms: Converter, fuel cell, proton-exchange membrane (PEM), reverse recovery, voltage clamped.

I. INTRODUCTION

INRECENT years, dc-dc converter switch steep voltage ratio are usually require din many industrial applications, e.g., the front-end stage for clean energy sources, the dc backup energy system for an uninterruptible power supply (UPS),high-intensity discharge (HID) lamps for automobile head lamps, And the telecommunication industry[1]–[3].The conventional boost converters cannot provide such a high dc-voltage ratio due to the losses associated with the inductor, filter capacitor, main switch, and output diode. Even for an extreme duty cycle, It will result in serious reverse-recovery problems and increase The rating of the output diode. As a result, the conversion efficiency is degraded, and the electromagnetic interference (EMI) problem is severe under this situation [4].In order to increase the conversion efficiency and voltage gain, many modified boost converter topologies have been investigated in the past decade[5]–[10].

Although voltage-clamped techniques are manipulated in the converter design to overcome the severe reverse-recovery problem of the output diode in high-level voltage applications, there still exist over large switch-voltage stresses, and the voltage gain is limited by the turn-ON time of the auxiliary switch [5], [6].da Silva et al. [7] presented a boost soft-single-switch converter, which has only one single active switch. It is able to operate with soft switching in a pulse width modulation (PWM) way without high voltage and current stresses. Unfortunately, the voltage gain is limited below four in order to achieve the function of

soft switching. In [8] and [9], coupled inductors were employed to provide ea high step-up ratio and to reduce the switch-voltage stress substantially, and the reverse-recovery problem of the output diode was also alleviated efficiently.

In this case, the leakage energy of the coupled inductor is another problem as the main switch was turned OFF. It will result in a high voltage ripple a cross the main switch due to the resonant phenomenon induced by the leakage current. In order to protect the switch devices, either a high-voltage-rated device with higher RDS (ON) or a snubber circuit is usually adopted to deplete the leakage energy. Consequently, the power-conversion efficiency will be degraded. Zhao and Lee [10] introduced a family of high-efficiency high-step-up dc-dc converters by only adding one addition diode and a small capacitor. It can recycle the leakage energy an

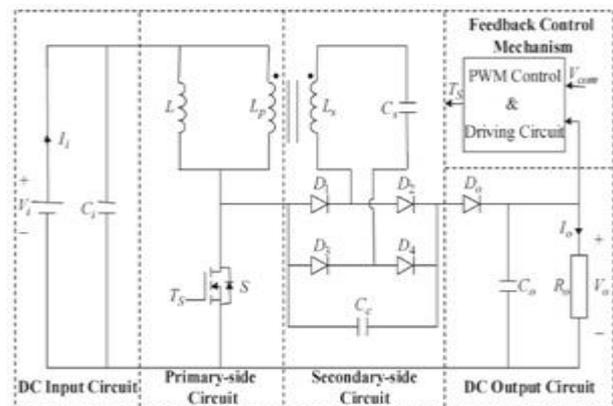


Fig. 1. System configuration of a high -efficiency voltage-clamped dc-dc converter.

Alleviate the reverse-recovery problem. However, a snubber circuit is still required in the output diode terminal with extra energy losses.

Nowadays, fuel cells are in the news because they appear to be one of the most efficient and effective solutions to the environmental pollution problem [11]–[17]. A fuel cell is an energy conversion device that produces electricity by electrochemically combining fuel (hydrogen) and oxidant (oxygen from the air) gases through electrodes, across an ion conduction electrolyte. This process produces much higher conversion efficiency than any conventional thermal-mechanical system, because it operates without combustion and extracts more electricity from the same amount of fuel. This system has the merits of high efficiency, energy security, reliability, pollution free, and quiet operations. Fuel cells have been known to science for more than 160 years and have recently become the subject of intense research and development. Up to the present, many demonstration projects have shown fuel-cell systems to be feasible for portable power, transportation, utility power and on-site power generation in a variety of building applications.

For portable power, a fuel cell with a fuel container can offer a higher-energy density and more convenience than conventional battery systems. Moreover, portable power packs using fuel cells can be lighter and smaller in volume for an equivalent amount of energy. In transportation applications, fuel cells offer higher efficiency and better part-load performance than conventional engines. In stationary power applications, low emissions permit fuel cells to be located in high-power requirement areas, where they can supplement the existing utility grid. Using fuel cells and hydrogen technology, electrical power can be delivered cleanly, efficiently and sustainably where and when required. The greatest research interests throughout the world have focused on proton-exchange membrane

(PEM) and solid oxide cell stacks. Specially, PEM fuel cell (PEMFC) has promising characteristics as follows: 1) the by-product waste is water; 2) low-temperature operation; and 3) they use a solid polymer as the electrolyte that reduces concerns related to construction, transportation, and safety issues [16]. Thus, it seems to be a good alternative source for distributed generation systems.

The aim of this study is to design a high-efficiency voltage clamped dc–dc converter with reduced reverse-recovery current and switch-voltage stress to provide a stable constant dc voltage. To achieve this goal, the manipulation of inductor and transformer is adopted to increase the voltage gain and to enhance the utility rate of the magnetic core. Moreover, the voltage-clamped technology is used for reducing the switch voltage stress and solving the reverse-recovery problem. In addition, the closed-loop control methodology is utilized in the proposed converter to overcome the voltage-drift problem of power source under the variation of loads. The prototype is developed for a PEMFC application requiring an output power of 310 W, an output voltage of 200 V, and an input voltage varying from 27 to 37.5 V. The remainder of this study is organized as follows. Section II presents the converter design and analyses in detail. Experimental results for a PEMFC power source with a 250-W nominal rating are provided to validate the effectiveness of the proposed power conversion system in Section III. Conclusions are drawn in Section IV.

II. CONVERTER DESIGN AND ANALYSES:

A newly designed converter topology is depicted in Fig. 1, where it contains five parts including a dc-input circuit, a primary-side circuit, a secondary-side circuit, a dc-output circuit, and a feedback-control mechanism. The major symbol representations are summarized as follows. V_i and I_i denote the dc-input voltage and current, and C_i is the input filter capacitor in the dc-input circuit. L_p represents the primary inductor of the transformer; L is the additional inductor in the primary-side circuit; and S is the main switch. L_s denote the secondary inductor of the transformer; C_s and C_c are the balanced capacitor and clamped capacitor in the secondary-side circuit; and $D_1, D_2, D_3,$ and D_4 are the rectifier diodes. V_o and I_o describe the output voltage and current; R_o is the output load; $D_o,$ and C_o are the output diode and filter capacitor in the output circuit. V_{com} and T_S are the output-voltage command and switch-driving signal in the feedback-control mechanism, respectively.

The equivalent circuit and state definition of the newly designed converter is depicted in Fig. 2, where the

transformer is modeled as an ideal transformer with a secondary leakage inductor (L_k). The turn's ratio of this ideal transformer is defined as

$$n = \frac{N_2}{N_1} \tag{1}$$

Where N_1 and N_2 are the primary and secondary winding turns. The additional inductor (L) is located in parallel with the primary side of the transformer. Moreover, the rectifier diodes ($D_1, D_2, D_3,$ and D_4) are connected between the primary and secondary sides of the transformer. The voltages across the additional inductor, the main switch, the ideal transformer primary and secondary winding, the secondary leakage inductor, the balanced capacitor, and the output diode are $v_L, v_{DS}, v_{Lp}, v_{Ls}, v_{Lk}, v_{Cs},$ and $v_{Do},$ respectively. The clamped capacitor C_c is assumed to be large enough to be viewed as a constant voltage source, V_{Cc} . The conductive voltage drops of the main switch

(S) and all diodes ($D_1, D_2, D_3, D_4,$ and D_o) are neglected to simplify the circuit analyses. The characteristic waveforms of the proposed high-efficiency converter are depicted in Fig. 3. In addition, Fig. 4 illustrates the operational modes in one switching cycle, and the detailed operation stages are described as follows.

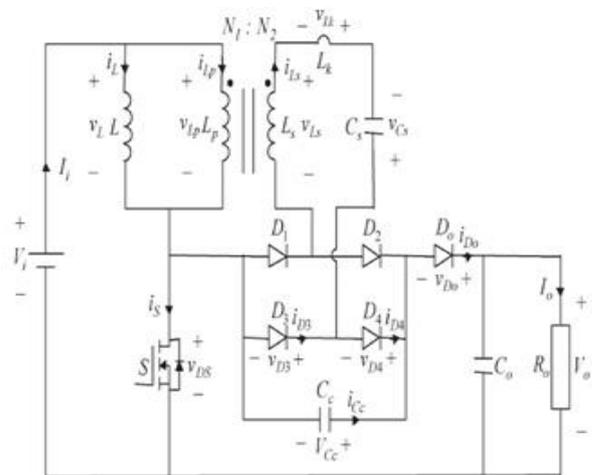


Fig. 2. Equivalent circuit.

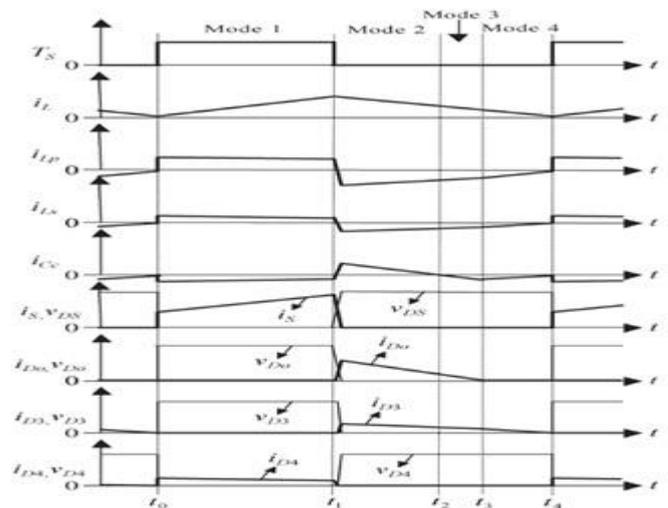


Fig. 3. Characteristic waveforms.

A. Mode 1 ($t_0 - t_1$) [Fig. 4(a)]

At time $t = t_0$, the main switch (S) is turned ON. At the sametime, the diodes ($D1$ and $D4$) become conducted, and other diodes ($D2$, $D3$, and D_0) are reverse biased. The additional inductor (L) and clamped capacitor (C_c) are linearly charged by the input-voltage source (V_i) through the transformer. Applying Kirchoff's law [4], the voltages of v_L , v_{Lp} , v_{Ls} , and v_{Lk} during this period can be expressed as

$$v_L = v_{Lp} = V_i \tag{2}$$

$$v_{Ls} = nV_i \tag{3}$$

$$v_{Lk} = VC_c - nV_i - v_{Cs} \tag{4}$$

According to (2)–(4), the rate of change of the additional inductor current (i_L), the primary-side current (i_{Lp}), and the secondary-side current (i_{Ls}) of the transformer can be represented as

$$\frac{di_L}{dt} = \frac{V_i}{L} \tag{5}$$

$$\frac{di_{Lp}}{dt} = \frac{VC_c - nV_i - v_{Cs}}{L_k} + \frac{V_i}{L_p} \tag{6}$$

$$\frac{di_{Ls}}{dt} = \frac{VC_c - nV_i - v_{Cs}}{L_k} \tag{7}$$

B. Mode 2 ($t_1 - t_2$) [Fig. 4(b)]

At time $t = t_1$, the main switch (S) is turned OFF. At this time, the diodes (D_2 , D_3 , and D_0) become forward biased to start conducting, and other diodes ($D1$ and $D4$) are reverse biased. The stored energy of the additional inductor (L) and clamped capacitor (C_c) in Mode 1 is released to output loads. Moreover, the transformer can be operated at four quadrants to enhance the utility rate of the magnetic core and to keep the clamped voltage (VC_c), since the additional inductor (L) sup supplies energy to the output terminal by way of the transformer. Applying Kirchoff's law [4], the voltage and current relations of each element during this mode can be described by

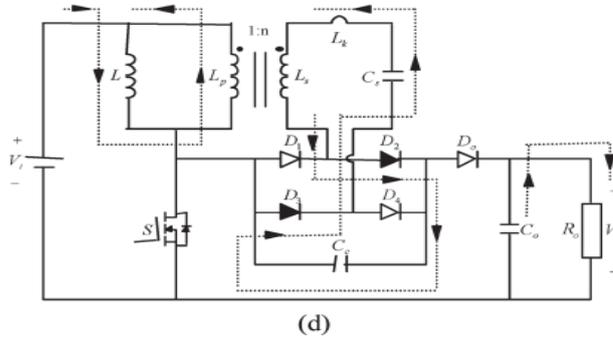
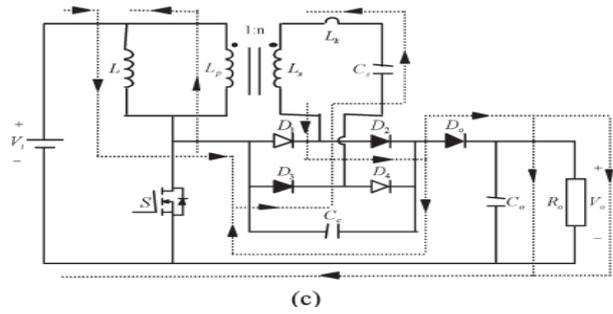
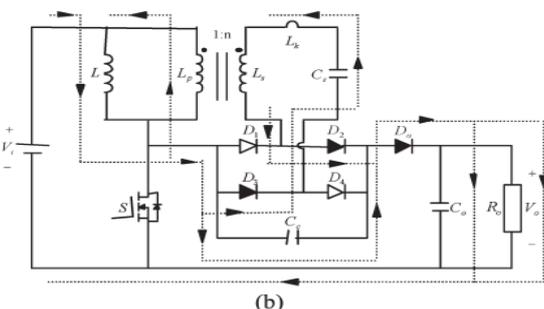
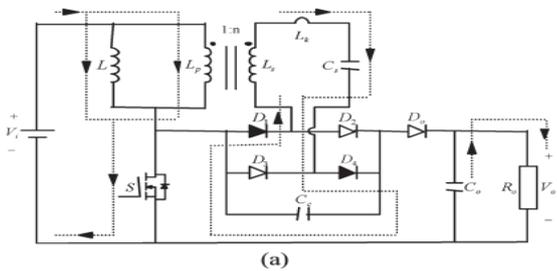


Fig.4.Operational modes: (a) mode 1 [$t_0 - t_1$]; (b) mode 2 [$t_1 - t_2$];(c) mode 3 [$t_2 - t_3$]; (d) mode 4 [$t_3 - t_4$].

$$v_L = v_{Lp} = V_i + VC_c - V_o \tag{8}$$

$$v_{Ls} = n(V_i + VC_c - V_o) \tag{9}$$

$$v_{Lk} = -VC_c - v_{Cs} - n(V_i + VC_c - V_o) \tag{10}$$

$$v_{DS} = V_i - V_L = V_o - VC_c < V_o \tag{11}$$

$$i_{D_0} = i_L + i_{Lp} = i_{C_c} - i_{Ls} \tag{12}$$

Where i_{D_0} is the current of the output diode D_0 ; i_{C_c} is the current of the clamped capacitor C_c . According to (11), the cutoff voltage of the main switch (S) is clamped at $V_o - VC_c$. Moreover, the main switch (S) with low-voltage-rated capacity can be selected since the switch-voltage stress (v_{DS}) is smaller than the output voltage (V_o). The selection of a low-voltage-rated device with lower $R_{DS(ON)}$ is useful for improving the conversion efficiency. Referring to (8)–(10), the rate of change of i_L , i_{Lp} and i_{Ls} is given by

$$\frac{di_L}{dt} = \frac{V_i + VC_c - V_o}{L} \tag{13}$$

$$\frac{di_{Lp}}{dt} = \frac{-VC_c - v_{Cs} - n(V_i + VC_c - V_o)}{L_k} + \frac{V_i + VC_c - V_o}{L_p} \tag{14}$$

$$\frac{di_{Ls}}{dt} = \frac{-VC_c - v_{Cs} - n(V_i + VC_c - V_o)}{L_k} \tag{15}$$

C. Mode 3 ($t_2 - t_3$) [Fig. 4(c)]

$$\frac{di_{C_c}}{dt} = \frac{V_i + VC_c - V_o}{L} + \frac{V_i + VC_c - V_o}{L_p} + 2 \left[\frac{-VC_c - v_{Cs} - n(V_i + VC_c - V_o)}{L_k} \right] \tag{16}$$

$$\frac{di_{D_o}}{dt} = \frac{V_i + V_{C_c} - V_o}{L} + \frac{V_i + V_{C_c} - V_o}{L_p} + \frac{-V_{C_c} - v_{C_s} - n(V_i + V_{C_c} - V_o)}{L_k} \quad (17)$$

$$\frac{di_{L_p}}{dt} = -\frac{di_L}{dt} = -\frac{V_i + V_{C_c} - V_o}{L} \quad (18)$$

$$\frac{di_{L_s}}{dt} = -\frac{V_i + V_{C_c} - V_o}{L} - \frac{V_i + V_{C_c} - V_o}{L_n} \quad (19)$$

$$v_{C_s} = \frac{nV_i(2d - 1)}{2(1 - d)} \quad (20)$$

$$V_{C_c} = \frac{nV_i}{2(1 - d)} \quad (21)$$

$$V_o = \frac{2 + n}{2(1 - d)} V_i \quad (22)$$

At time $t = t2$, the residual energy of the clamped capacitor (C_c) is discharged entirely, i.e., $i_{C_c}(t2) = 0$. Immediately, the clamped capacitor (C_c) is charged by the energy of the additional inductor (L) through the transformer, and the rate of change of the clamped-capacitor current (i_{C_c}) can be denoted as Moreover, the stored energy of the additional inductor (L) is released continuously to the output terminal by way of the transformer. The rate of charge of i_{D_o} is given by

$$v_{DS} = \frac{V_i}{(1 - d)} \quad (23)$$

$$v_{DS} = \frac{2V_o}{(2 + n)} \quad (24)$$

D. Mode 4 ($t3 - t4$) [Fig. 4(d)]

At time $t = t3$, the clamped-capacitor current (i_{C_c}) equals to the secondary-side current (i_{L_s}) of the transformer, and the output diode current (i_{D_o}) decays to 0, i.e., $i_{D_o}(t3) = 0$. During this period, the voltage of the output diode (v_{D_o}) Maintains the zero status until the main switch (S) is turned ON. Moreover, the magnitude of the additional inductor current (i_L) is equal to the one of the primary-side current (i_{L_p}). According to (13) and (14), the rate of change of i_{L_p} and i_{L_s} can be represented as Since the secondary leakage inductor (L_k) and the change rate of i_{L_s} in the transformer are very small, the voltage of the secondary leakage inductor (v_{L_k}) can be neglected. According to the concept of the zero average voltage across the inductor over one period [4], the voltages of v_{C_s} , V_{C_c} , and V_o for steady state operation can be described via (2), (4), (8), and (10) as.

Since the voltage difference may be caused by the secondary inductor of the transformer, as $d = 0.5$, the major function of the balanced capacitor (C_c) is used for keeping the cutoff voltages of the rectifier diodes ($D1$, $D2$, $D3$, and $D4$) balanced. Moreover, it also can avoid the overlarge current that passed through the rectifier diodes. According to (22), the voltage gain can be tuned by regulating the turn's ratio (n) in the transformer to overcome the boost- ratio limitation of the conventional converter. In addition, the

switch-voltage stress (v_{DS}) can be calculated(11),and (22) as

Where d is the duty cycle of the main switch (S). Continuously, the main switch (S) is turned ON at time $t = t4$ to begin the next switching cycle.

By analyzing (24), the switch-voltage stress (v_{DS}) is not related to the dc-input voltage (V_i) and duty cycle (d) if the values of the output voltage (V_o) and the turns ratio (n) are fixed. Thus, it can ensure that the sustainable voltage of the main switch (S) is constant. As long as the dc-input voltage is not higher than the rated voltage of the main switch, the high-efficiency voltage clamped dc-dc converter can be applied well to the low-voltage power sources even with large voltage variations, e.g., fuel cell, solar cell, etc.

Fuel-cell generation systems have been receiving more attention in the last years due to the advantages of high-conversion efficiency, low aggression to the environment, no moving parts, and superior reliability and durability. Owing to the electrochemical reaction, fuel cell has the power quality of low voltage and high current. However, the fuel-cell stack with high output voltage is difficult to fabricate and it may be failure when any single cell is inactive. Besides, the output voltage is varied easily with respect to the load variations. In order to satisfy the requirement of high-voltage demand, a stable boost converter with high voltage gain and superior conversion efficiency is necessary to utilize the fuel-cell energy more efficiently. The validity of the proposed converter is verified by the following experimental results via an example of a PEMFC power source.

III. EXPERIMENTAL RESULTS

In order to verify the effectiveness of the designed converter topology, the clean energy of a PEMFC system is utilized for the low-voltage power source in the proposed high-efficiency voltage-clamped dc-dc converter, and its application circuit is depicted in Fig. 5. The PEMFC system used in this study is the PowerPEM™-PS250 manufactured by the H power Company. It is a dc power source with 250-W dc nominal power rating.

The system operates on an ambient air and clean pressurized hydrogen fuel. The fuel-cell system consists of a (40) cell stack of the PEM type, mechanical auxiliaries, and electronic control module. In experimentation, the high-efficiency voltage-clamped dc-dc converter is designed to operate from the fuel-cell variability dc input, $V_i = 27-37.5$ V, to deliver a constant dc output, $V_o = 200$ V, with the maximal capability of output power, $P_{o,max} = 330$ W. If the maximal value of main switch voltage (v_{DS}) is arranged for clamping at 50 V, the turns ratio can be determined as $n = (2V_o/v_{DS(max)}) - 2 = 6$ according to (24). As can be seen from Figs. 3 and 4, the voltage stress of the output diode (v_{D_o}) is the same as the switch-voltage stress. In addition, the voltage stresses of rectifier diodes (v_{D1} , v_{D2} , v_{D3} , and v_{D4}) can be calculated via (21) and (23) as $n v_{DS}/2 = 150$ V. For conservative consideration, the main switch (FQI90N08, 80 V), the output diode (Schottky diode SR20100, 100 V), and the rectifier diodes (Schottky diode SR20200, 200 V) are adopted in the experimental converter.

In order to solve the problem of the fuel-cell output voltage varied with the variations of loads, the proposed converter with dc-voltage feedback control is utilized to ensure the system stability, and a PWM control IC TL494 is adopted to

achieve this goal of feedback control. The prototype with the following

Specifications are designed in this section to illustrate the design procedure given in Section II:

Switching frequency $f_s = 100$ kHz;

Turns ratio $n = 6$;

Additional inductor $L = 5.9$ μ H;

Primary inductor of transformer $L_p = 213.6$ μ H

Secondary inductor of transformer $L_s = 7689.6$ μ H;

Secondary leakage inductor $L_k = 0.6$ μ H;

Balanced capacitor $C_s = 4 \times 6.8$ μ F;

Clamped capacitor $C_c = 6 \times 4.7$ μ F;

Input filter capacitor $C_i = 3300$ μ F;

Output filter capacitor $C_o = 3 \times 4.7$ μ F;

Main switch S : FQI90N08 (80 V,

RDS (ON) = 16 m Ω);

Output diode D_o : Schottky diode

SR20100 (100 V, 20 A);

Rectifier diodes D_1, D_2, D_3, D_4 :

Scotty diode SR20200 (200 V, 20 A).

Fig. 5 depicts the experimental voltage and current curves of the main switch (S) at 310-W output power. As can be seen from this figure, the shaken switch voltage at the beginning is caused by the line inductor when the switch is turned OFF. Fortunately, the steady state of this switch-voltage stress is about 50 V due to the utilization of voltage-clamped technique, and it is much smaller than the output voltage, $V_o = 200$ V. It has the merit of selecting a low-voltage-rated device in order to reduce the conduction loss of the switch.

The experimental current waveforms of the additional inductor (L), in parallel with the transformer, primary inductor of transformer (L_p), and secondary inductor of transformer (L_s) at 310-W output power, are depicted in Fig. 5(c). By observing the currents of i_{Lp} and i_{Ls} , it is obvious that the transformer is manipulated during the four-quadrant operation so that the utility rate of the magnetic core is improved to exhibit the transformer characteristics completely. The experimental voltage and current responses of the diodes (D_o, D_3 , and D_4) at 310-W output power are depicted in Fig. 5. From these results, the reverse-recovery currents in these diodes are small to give the credit to the utilization of Schottky diodes with extremely low switching and conduction losses. Thus, it can alleviate the reverse-recovery problem for further raising the conversion efficiency. As can be seen from Fig. 5(a) and (b),

The balanced capacitor (C_s) can be used for balancing the current and cutoff voltage of the diodes (D_3 and D_4) when the condition of $d = 0.5$ holds. For verifying the voltage-clamped property, the experimental voltage responses of the output voltage (V_o), clamped capacitor (C_c), output diode (D_o), and main switch (S) at 310-W output power are depicted. As can be seen from this figure, the output voltage, $V_o = 200$ V, is strode mainly across the clamped capacitor in the secondary-side circuit (i.e., $V_{C_c} = 150$ V). Thus, the switch-voltage stress and the cutoff voltage of the output diode are clamped at about 50 V. In order to examine the robust performance of the proposed converter scheme, the experimental results of the converter output voltage (V_o), output current (I_o), and the PEMFC output current (I) under the step load variation between no load (0 W) and full load (310 W) are depicted Fig. 10.

According to Fig. 10, the converter output voltage, $V_o = 200$ V, is insensitive to the variation of loads due to the closed-loop control, and the output current ripple is also slightly extreme as a result of the high switching frequency. Fig. 11 summarizes the conversion efficiency of the proposed converter and the PEMFC output voltage under different output powers. From the experimental results, the measure of efficiency of the proposed converter operating at 310-W output power is 95.6%, and the maximal efficiency is 96.5% at 190-W output power. The above experimental results agree well with those obtained from the design procedure given in Section II. However, slight differences in these results are attributed to the factor of system uncertainties in practical applications.

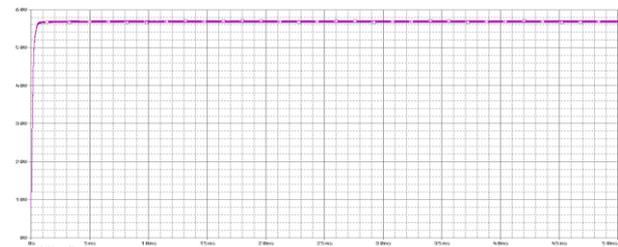


Fig 5 (a)output voltage

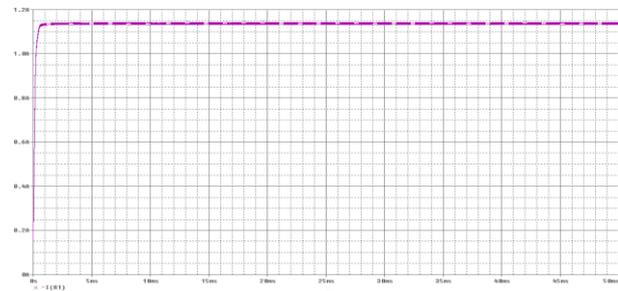


Fig 5 (b)output current:

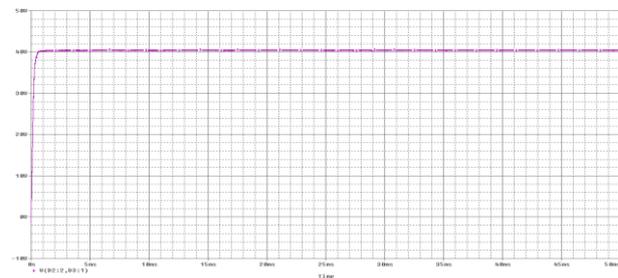


Fig 5 (c) clamped capacitor voltage

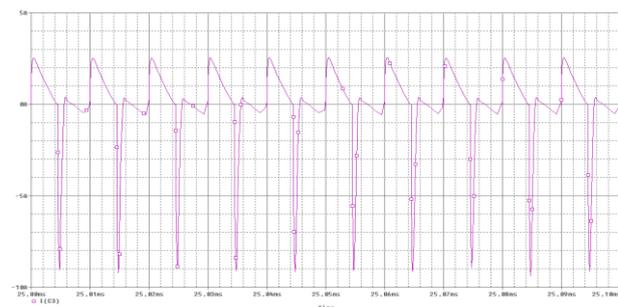


Fig 5 (d) clamped capacitor current

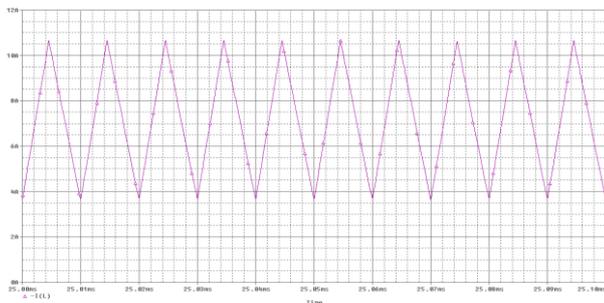


Fig 5 (e) Inductor current:

IV. CONCLUSION

This paper has successfully developed a high-efficiency voltage-clamped dc-dc converter with reduced reverse recovery current and switch-voltage stress, and this converter has been applied well to a PEMFC system with a power quality of low voltage and high current. According to the experimental results, the maximal efficiency was measured to be over 96%, which is comparatively higher than the conventional converter with the same voltage gain. The newly designed converter circuit has the following improvements compared to the previous work.

- 1) It can select the main switch with lower sustainable voltage for alleviating the switch conduction loss due to the utilization of voltage-clamped technique.
- 2) All diodes in this circuit topology are Schottky diodes with the reduction of switching and conduction losses.
- 3) The additional inductor is used for providing the reverse current path of the transformer to raise the utility rate of the magnetic core.
- 4) Additional snubber circuits for absorbing the voltage spikes in the diodes are not required to further cut down the manufacture cost.
- 5) There is no circulating current to overcome the problem of degenerate efficiency under slight loads.
- 6) The voltage-drift problem of power source under the variation of loads can be solved by the closed-loop control methodology.

This new converter topology provides designers with an alternative choice to convert renewable energy efficiently, and it also can be extended easily to other power-conversion systems for satisfying high-voltage demands.

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